

Radio Wave Propagation Characteristics in FMCW Radar

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ABSTRACT

FMCW Radar (Frequency Modulated Continuous Wave Radar) is used for various purposes, such as atmospheric Remote Sensing, inter-vehicle ranging, etc. FMCW radar systems are usually very compact, relatively cheap in purchase as well as in daily use, and consume little power. In this paper, FMCW radar determines a target range by measuring the beat frequency between a transmitted signal and the received signal from the target, and Combines between PO and radar single. The approach based on frequency domain physical optics for the scattering estimation and the linear system modeling for the estimation of time domain response, and FMCW Radar signal processing.

Keywords: Radio Wave, FMCW Radar, Cloud Profiling Radar

1. Introduction

The FMCW radar has to adjust the range of frequencies of operation to suit the material and targets under investigation. The transceiver generates a signal of linearly increasing frequency for the frequency-sweep period. The signal propagates from the antenna to a static target and back. The value of the received-signal frequency compared to the transmitted-signal frequency is proportional to the propagation range. The main advantages of the FMCW radar are the wider dynamic range, lower noise figure and higher mean powers that can be radiated. In addition a much wider class of antenna is available for use by the designer.

The further advantage of FMCW radar is its ability to adjust the range of frequencies of operation to suit the material and targets under investigation if the antenna has an adequate pass-band of frequencies. This radar system mixes the wave reflected by a target object and part of the radiated wave to obtain a beat signal that contains distance and speed components. For large scatterer, the physical-optics approximation is an efficient method in the frequency domain [1,2]. This physical optics (PO) approximation is initially applied in the frequency-domain with the inverse Fourier transform [3], [4], [5], [6]. With FMCW, the high-frequency circuitry for beat signal detection is relatively simple and distance can be directly obtained. By mixing the received FMCW and transmitted FMCW signals, the system obtains a beat signal having a frequency f_b .

2. The Principles of the FMCW Radar

The principle of the FMCW radar is shown in Figure 1. Transmitted signal from one of the antennas is reflected, and is received by the other antenna with delay time T_o relative to the original transmitted signal. Mixing the received and transmitted frequencies, the beat frequencies f_b are observed in the spectra.

The time takes for the signal to travel the two-way distance between the target and the radar is T_o , hence [7], [8]:

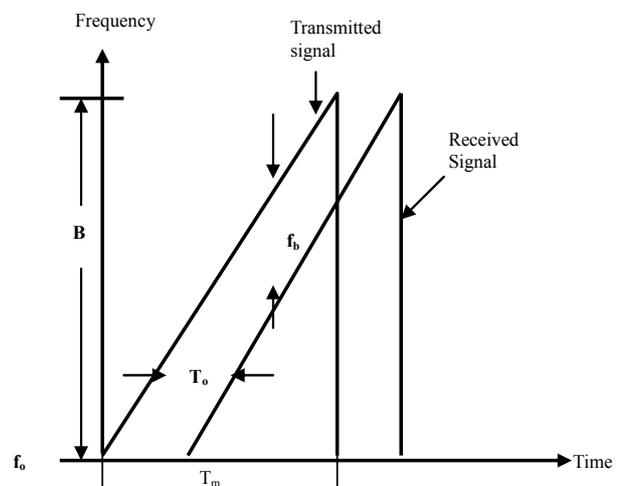


Figure 1. Principle of the FMCW radar

$$T_o = \frac{2R}{c} \quad (1)$$

From the geometry of transmit and receive waveforms we can derive a relationship between the beat frequency f_b , the range R , and c is the velocity of light.

From Figure 1, we can see,

$$\frac{T_o}{T_m} = \frac{f_b}{B} \quad (2)$$

Substituting (1) in (2), we get

$$f_b = \frac{2RB}{cT_m} \quad (3)$$

3. Scattered Wave from Radar Target

3.1 Frequency Domain Physical Optics

For a perfectly conducting body, the frequency-domain PO-induced current distribution over the illuminated surface is [9,10,11]:

$$\bar{j}_s^{po}(\bar{R}, \omega) = 2\hat{n} \times \bar{H}^{inc}(\bar{R}, \omega) \quad (4)$$

where \hat{n} is the unit vector normal to the surface \bar{R} and $\bar{H}^{inc}(\bar{R}, \omega)$ is the incident magnetic field with angular frequency ω .

The frequency-domain scattered field is obtained by calculating the integral over the illuminated surface using

$$H(\omega) = \frac{\eta_o}{4\pi F_c(\omega) V_i(\omega)} \sum_k \frac{1}{|\bar{R} - \bar{R}_k|} \{2\hat{n} \times \bar{H}^{inc}(\bar{R}_k, \omega)\} e^{-jk_o|\bar{R} - \bar{R}_k|} \Delta S_k \quad (8)$$

where $F_c(\omega)$ is the Complex antenna factor.

3.2 Treatment of FMCW Signal

Instantaneous frequency $f_i(t)$, is given as

$$f_i(t) = \left(f_o + \frac{t}{T_m} B \right) \quad (0 \leq t \leq T_m)$$

and the instantaneous phase $\varphi_i(t)$, is defined as

$$\varphi_i(t) = 2\pi \int_0^t f_i(\tau) d\tau = 2\pi f_o t + \pi \frac{B}{T_m} t^2 \quad (9)$$

Using Equation (9), the FMCW signal waveform is defined as

$$v_i(t) = V_i \text{Cos} \left(2\pi f_o t + \pi \frac{B}{T_m} t^2 \right) \quad (10)$$

The output of mixer $V_{FMCW1}(t)$ is expressed as

$$V_{FMCW1}(t) = v_i(t) v_o(t) \quad (11)$$

The output waveform $v_o(t)$ is

$$v_o(t) = v_i(t) * h(t)$$

when $h(t)$ is a sample delay of T_o , i.e.

the free space Green's function:

$$\bar{H}^{inc}(\bar{R}, \omega) \bar{E}^{po}(\bar{R}, \omega) = -\eta_o \iint_S \bar{j}_s^{po}(\bar{R}', \omega) \frac{e^{-jk_o|\bar{R} - \bar{R}'|}}{4\pi|\bar{R} - \bar{R}'|} ds \quad (5)$$

where the vector \bar{R}' locates the integration point on the scatterer surface, k_o is the wave number, $c = \frac{2\pi f}{k_o}$

is the velocity of the light and η_o is the intrinsic free space impedance, and $\bar{j}_s^{po}(\bar{R}', \omega)$ is the surface-current distribution.

The frequency transfer function $H(\omega)$ is defined as

$$H(\omega) = \frac{V_o(\omega)}{V_i(\omega)} \quad (6)$$

where $V_i(\omega)$ is the input waveform in frequency domain physical optics, this is just a magnitude of the source.

The output Voltage $V_o(\omega)$ is calculated from $E^{po}(R, \omega)$ by considering the receiver antennas as [12,13],

$$V_o(\omega) = \frac{E^{po}(R, \omega)}{F_c(\omega)} \quad (7)$$

$$h(t) = \delta(t - T_o) \quad (12)$$

Therefore, mixer output signal is

$$V_{FMCW1}(t) = v_i(t) v_i(t - T_o) \quad (13)$$

where

$$v_i(t - T_o) = V_i \text{Cos} \left[2\pi f_o(t - T_o) + \pi \frac{B}{T_m}(t - T_o)^2 \right] \quad (14)$$

From Equations (10) and (11) we can calculate:

$$V_{FMCW1}(t) = \frac{V_i^2}{2} \{ \text{Cos}(4\pi f_o t - 2\pi f_o T_o + \pi \frac{B}{T_m}(2t^2 - 2T_o t + T_o^2)) + \text{Cos}(2\pi f_o T_o + \pi \frac{B}{T_m}(2T_o t - T_o^2)) \} \quad (15)$$

The first Cos term describes a linearly increasing FM signal (chirp) at about twice the carrier frequency with a phase shift that is proportional to the delay time T_o . This term is generally filtered out.

The second Cos term:

$$V_{FMCW2}(t) = \frac{V_i^2}{2} \text{Cos} \left(2\pi f_o T_o + \pi \frac{B}{T_m}(2T_o t - T_o^2) \right) \quad (16)$$

describes a beat signal at a fixed frequency $f_b = \frac{B}{T_m} T_o$.

3.3 Combination of PO and Radar Single Processing

As $h(t)$ given in section 3.2 is just an idealized model, more realistic $h(t)$ obtained by PO in section 3.1, Equation (12) shall be used.

However, Equation (6) is given in frequency domain $H(\omega)$, and it shall be Inverse Fourier transformed

$$h(t) = \frac{1}{2\pi} \int_{-\infty}^{\infty} H(\omega) e^{j\omega t} d\omega \quad (17)$$

It is sufficient that $H(\omega)$ is computed only within the source frequency range, i.e. $f_o \leq f \leq f_o + B$. Outside the band, $H(\omega)$ can be assumed zero, $V_i(\omega)$ is also zero in this region.

In reality, Fourier transform shall be executed numerically. Let us assume the sampling interval ΔT which shall satisfy the following relation

$$\Delta T \leq \frac{1}{2(f_o + B)} \quad (18)$$

$$f_s = \frac{1}{\Delta T} \quad (19)$$

$$f_o = N_L f_s \quad (20)$$

$$f_o + B \leq (N_L + N_B) f_s \quad (21)$$

where f_s is a sampling frequency, N_L , and N_B are some certain integers.

Now $v_i(t)$ is denoted as $v_i(l\Delta T)$, and $h(n\Delta T)$ is given as,

$$h(n\Delta T) = \frac{f_s}{4(N_L + N_B)} \left(\sum_{m=N_L}^{N_L+N_B} (H(m 2\pi f_s) e^{jm 2\pi f_s n\Delta T} + H^*(m 2\pi f_s) e^{-jm 2\pi f_s n\Delta T}) \right) \quad (22)$$

Convolution (11) is now implemented as,

$$v_o(l\Delta T) = \Delta T \sum_{n=0}^{2(N_L+N_B)} v_i((l-n)\Delta T) h(n\Delta T) \quad (23)$$

Substituting from (23) and (10) in (13), we can get

$$V_{fmcw1}(t) = V_i^2 \text{Cos}(2\pi f_o t + \pi \frac{B}{T_m} t^2) \Delta T \sum_{n=0}^{2(N_L+N_B)} \text{Cos}(2\pi f_o ((l-n)\Delta T) + \pi \frac{B}{T_m} ((l-n)\Delta T)^2) h(n\Delta T) \quad (24)$$

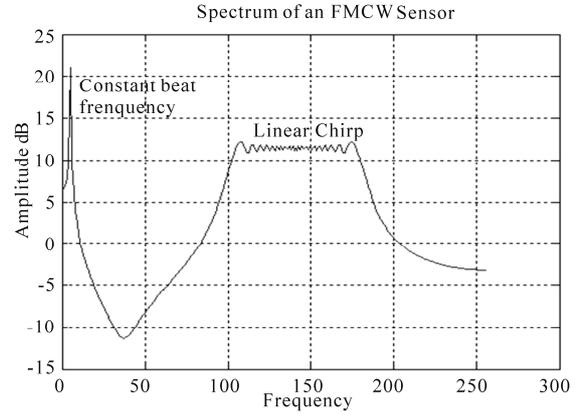


Figure 2. Frequency domain representation of FMCW sensor output

where $N_L \leq m \leq (N_L + N_B)$,

Now, we use Fourier Transformation, we get

$$V_{FMCW1}(f) = \frac{V_i^2}{2} \text{Cos}(2\pi f_c \tau_{fb} + \pi \frac{B}{T_m} \tau_{fb}^2) \Delta T \int_0^{\infty} \text{Cos}(2\pi f_o ((l-n)\Delta T) + \pi \frac{B}{T_m} ((l-n)\Delta T)^2) h(n\Delta T) e^{-j(m 2\pi f - n \Delta T) \Delta T} \Delta T \quad (25)$$

And also we can get

$$V_{FMCW2}(f) = \frac{V_i^2}{2} \text{Cos}(2\pi f_c \tau_{fb} + \pi \frac{B}{T_m} \tau_{fb}^2) \quad (26)$$

describes a beat signal at a fixed frequency $f_b = \frac{B}{T_f} \tau$.

It can be seen that the signal frequency is directly proportional to the time delay time τ , and hence is directly proportional to the round trip time to the target.

4. Conclusions

This paper presents the time domain linear system analysis for FMCW radar response by performing the inverse Fourier transform over the frequency-domain scattered field which obtained by calculating the integral over the illuminated surface using the free space Green's function. Then we got the received FMCW signal and transmitted FMCW signal, the product detection is implemented to get the beat signal. The Fourier transform is used to find the beat frequency.

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